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Nash Region of the Linear Deterministic Interference Channel with Noisy Output Feedback

Victor Quintero, Samir M. Perlaza, Jean-Marie Gorce, and H. Vincent Poor

Abstract—In this paper, the ϵ-Nash equilibrium (ϵ-NE) region of the two-user linear deterministic interference channel (IC) with noisy channel-output feedback is characterized for all ϵ > 0. The ϵ-NE region, a subset of the capacity region, contains the set of all achievable information rate pairs that are stable in the sense of an ϵ-NE. More specifically, given an ϵ-NE coding scheme, there does not exist an alternative coding scheme for either transmitter-receiver pair that increases the individual rate by more than ϵ bits per channel use. Existing results such as the ϵ-NE region of the linear deterministic IC without feedback and with perfect output feedback are obtained as particular cases of the result presented in this paper.

Index Terms—Nash equilibrium, Linear Deterministic Interference Channel.

I. SYSTEM MODEL

Consider the two-user decentralized linear deterministic interference channel with noisy channel-output feedback (D-LD-IC-NOF) depicted in Figure 1. For all i ∈ {1, 2}, with j ∈ {1, 2} \ {i}, the number of bit-pipes between transmitter i and its intended receiver is denoted by n_{ii}; the number of bit-pipes between transmitter i and its non-intended receiver is denoted by n_{ij}; and the number of bit-pipes between receiver i and its corresponding transmitter is denoted by n_{ji}. These six non-negative integer parameters describe the D-LD-IC-NOF in Figure 1.

At transmitter i, the channel-input \( X_{i,n} \) at channel use n, with n ∈ {1, 2, ..., N_i}, is a q-dimensional binary vector \( X_{i,n} = (X_{i,n}^{(1)}, X_{i,n}^{(2)}, ..., X_{i,n}^{(q)}) \in \mathbb{X}_i \), with \( \mathbb{X}_i = \{0,1\}^q \),

\[
q = \max \{n_{ii}, n_{ji}, n_{ji}, n_{ji}, n_{ji}, n_{ji}\}, \tag{1}
\]

and \( N_i \in \mathbb{N} \) is the block-length of transmitter-receiver pair i. At receiver i, the channel-output \( Y_{i,n} \) at channel use n, with n ∈ {1, 2, ..., max(\( N_{j_1}, N_{j_2} \))}, is also a q-dimensional binary vector \( Y_{i,n} = (Y_{i,n}^{(1)}, Y_{i,n}^{(2)}, ..., Y_{i,n}^{(q)}) \). Let S be a q×q binary lower shift matrix. The input-output relation during channel use n is given by

\[
Y_{i,n} = S_{q-n_i} X_{i,n} + S_{q-n_i} X_{j,n}, \tag{2}
\]

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Fig. 1. Two-user linear deterministic interference channel with noisy channel-output feedback at channel use n.

where \( X_{i,n} = (0,0,\ldots,0)^T \) for all n > \( N_i \). The feedback signal \( \hat{Y}_{i,n} \) available at transmitter i at the end of channel use n is

\[
\hat{Y}_{i,n} = S_{q-n_i} Y_{i,n} + S_{q-n_i} Y_{j,n}, \tag{3}
\]

where d is a finite delay, additions and multiplications are defined over the binary field, and \((\cdot)^+\) is the positive part operator.

Without any loss of generality, the feedback delay is assumed to be equal to one channel use. Let \( \mathcal{W}_i \) be the set of message indices of transmitter i. Transmitter i sends the message index \( W_i \in \mathcal{W}_i \) by transmitting the codeword \( X_i = (X_{i,1}, X_{i,2}, ..., X_{i,N_i}) \in \mathbb{X}_{i,N_i} \), which is a binary q × \( N_i \) matrix. The encoder of transmitter i can be modeled as a set of deterministic mappings \( f_{i,1}^{(N_i)}(W_i, N_i) \), with \( f_{i,1}^{(N_i)} : W_i \times N_i \to \{0,1\}^q \) and for all n ∈ {2, 3, ..., \( N_i \)}, \( f_{i,n}^{(N_i)} : W_i \times N_i \times \{0,1\}^{q \times (n-1)} \to \{0,1\}^q \), such that

\[
X_{i,1} = f_{i,1}^{(N_i)}(W_i, \Omega_i) \tag{4a}
\]

\[
X_{i,n} = f_{i,n}^{(N_i)}(W_i, \Omega_i, \hat{Y}_{i,1}, \hat{Y}_{i,2}, ..., \hat{Y}_{i,n-1}) \tag{4b}
\]

where \( \Omega_i \) is a randomly generated index known by both transmitter i and receiver i, while unknown by transmitter j and receiver j. The decoder of receiver i is defined by a deterministic function \( \psi_i^{(N_i)} : \{0,1\}^{q \times N_i} \times \mathbb{N} \to W_i \). At the end of the communication, receiver i uses the q × N binary matrix \( (\hat{Y}_{i,1}, \hat{Y}_{i,2}, ..., \hat{Y}_{i,N_i}) \) and \( \Omega_i \) to obtain an estimate \( \hat{W}_i \in \mathcal{W}_i \) of the message index \( W_i \), i.e.,
The set $K$ utility function of player transmit-receive configuration as described in Section I. The following section models this interaction using tools from mutual interference. This reveals the competitive interaction $\eta$-bit error probabilities $p_i(s_1, s_2)$, denoted by $\eta$, can be made arbitrarily small by letting the block-lengths $N_1$ and $N_2$ grow to infinity.

The aim of transmitter $i$ is to autonomously choose its transmit-receive configuration $s_i$, in order to maximize its achievable rate $R_i$. Note that the rate achieved by transmitter-receiver $i$ depends on both configurations $s_1$ and $s_2$ due to mutual interference. This reveals the competitive interaction between both links in the decentralized interference channel. The following section models this interaction using tools from game theory.

II. THE TWO-USER INTERFERENCE CHANNEL AS A GAME

The competitive interaction between the two transmitter-receiver pairs in the decentralized interference channel can be modeled by the following game in normal-form: $G = (K, \{A_k\}_{k \in K}, \{u_k\}_{k \in K})$. The set $K = \{1, 2\}$ is the set of players, that is, the set of transmitter-receiver pairs. The sets $A_1$ and $A_2$ are the sets of actions of players 1 and 2, respectively. An action of a player $i \in K$, which is denoted by $s_i \in A_i$, is basically its transmit-receive configuration as described in Section I. The utility function of player $i$ is $u_i : A_1 \times A_2 \rightarrow R_+$ and it is defined as the information rate of transmitter $i$, $u_i(s_1, s_2) = \left\{ \begin{array}{ll} R_i = \frac{M}{N_i} & \text{if } p_i(s_1, s_2) < \epsilon \\ 0 & \text{otherwise} \end{array} \right.$, where $\epsilon > 0$ is an arbitrarily small number.

This game formulation was first proposed in [1] and [2]. A class of transmit-receive configurations $s^* = (s_1^*, s_2^*) \in A_1 \times A_2$ that are particularly important in the analysis of this game is referred to as the set of $\eta$-Nash equilibria ($\eta$-NE), with $\eta > 0$. This type of configuration satisfies the following definition.

Definition 2 ($\eta$-Nash equilibrium): In the game $G = (K, \{A_k\}_{k \in K}, \{u_k\}_{k \in K})$, an action profile $(s_1^*, s_2^*)$ is an $\eta$-Nash equilibrium if for all $i \in K$ and for all $s_i \in A_i$, there exists an $\eta > 0$ such that $u_i(s_i, s_2^*) \leq u_i(s_1^*, s_2^*) + \eta$. Let $(s_1^*, s_2^*)$ be an $\eta$-Nash equilibrium action profile of the game in (6). Then, none of the transmitters can increase its own information transmission rate more than $\eta$ bits per channel use by changing its own transmit-receive configuration and keeping the average bit error probability arbitrarily close to zero. Note that for $\eta$ sufficiently large, from Definition 2, any pair of configurations can be an $\eta$-NE. Alternatively, for $\eta = 0$, the classical definition of Nash equilibrium ($\eta = 0$), then each individual configuration is optimal with respect to each other. Hence, the interest is to describe the set of all possible $\eta$-NE rate pairs $(R_1, R_2)$ of the game in (6) with the smallest $\eta$ for which there exists at least one equilibrium configuration pair. The set of rate pairs that can be achieved at an $\eta$-NE is known as the $\eta$-Nash equilibrium region.

Definition 3 ($\eta$-NE Region): Let $\eta > 0$ be fixed. An achievable rate pair $(R_1, R_2)$ is said to be in the $\eta$-NE region of the game $G = (K, \{A_k\}_{k \in K}, \{u_k\}_{k \in K})$ if there exists a pair $(s_1^*, s_2^*) \in A_1 \times A_2$ that is an $\eta$-NE and the following holds: $u_1(s_1^*, s_2^*) = R_1$ and $u_2(s_1^*, s_2^*) = R_2$.

The following section characterizes the $\eta$-NE region (Def. 3) of the two-user D-LD-IC-NOF in (6), denoted by $\mathcal{N}_\eta = (\overline{n}_{11}, \overline{n}_{12}, n_{21}, \overline{n}_{22})$, for fixed parameters $(\overline{n}_{11}, \overline{n}_{12}, n_{21}, \overline{n}_{22}) \in \mathbb{N}^8$ and for all $\eta > 0$.

III. MAIN RESULTS

The $\eta$-NE region is characterized in terms of two regions: the capacity region, denoted by $C(\overline{n}_{11}, \overline{n}_{12}, n_{21}, \overline{n}_{22})$ and a convex region, denoted by $B(\overline{n}_{11}, \overline{n}_{12}, n_{21}, \overline{n}_{22})$. In the following, the tuple $(\overline{n}_{11}, \overline{n}_{12}, n_{21}, \overline{n}_{22})$ is used only when needed.

The capacity region $C$ of the two-user LD-IC-NOF is described in Theorem 1 in [4], which is a generalization of previous works in [5] and [6]. For all $\eta > 0$, the convex region $B_\eta$ is defined as follows: $B_\eta = \left\{ (R_1, R_2) : L_i \leq R_i \leq U_i, \text{ for all } i \in \{1, 2\} \right\}$, (10) where, $L_i = \left( (\overline{n}_{ii} - n_{ij})^+ - \eta \right)^+$ and $U_i = \max (\overline{n}_{ii}, n_{ij}) - \left( \min ((\overline{n}_{jj} - n_{jj})^+, n_{jj}) \right) + \eta$ - $\left( \min ((\overline{n}_{jj} - n_{jj})^+, n_{jj}) - (\max (\overline{n}_{jj}, n_{jj}) - \eta_{jj})^+ \right)^+, (11a)$ $\eta$ + $\eta$, with $i \in \{1, 2\}$ and $j \in \{1, 2\} \setminus \{i\}$. Theorem 1 uses the region $B_\eta$ in (10) and the capacity region $C$ to describe the $\eta$-NE region $\mathcal{N}_\eta$.

Theorem 1: Let $\eta > 0$ be fixed. The $\eta$-NE region $\mathcal{N}_\eta$ of the two-user D-LD-IC-NOF with parameters $\overline{n}_{11}, \overline{n}_{12}, n_{21}, \overline{n}_{22}, n_{12}, \overline{n}_{22}$, is $\mathcal{N}_\eta = C \cap B_\eta$.

Figure 2 shows the capacity region $C$ and the $\eta$-NE region $\mathcal{N}_\eta$ of a channel with parameters $\overline{n}_{11} = 7, \overline{n}_{12} = 6, n_{12} = 4, n_{21} = 4$ and different values for $\overline{n}_{11}$ and $\overline{n}_{22}$, with $\eta$ chosen arbitrarily small. Note that when $\overline{n}_{11} \in \mathbb{N}$.
\(R_1\) (bits/channel use) 
\[0, 1, 2, 3, 4\]
\(R_2\) (bits/channel use) 
\[0, 1, 2, 3, 4\]
\(C\) with feedback
\(C\) without feedback
\(N\) with feedback
\(N\) without feedback
(b) (c)

Fig. 2. Capacity region \(C(7, 6, 4, 0, 0)\) (thin blue line) and \(\eta\)-NE region \(N_\eta(7, 6, 4, 0, 0)\) (thick black line) with \(\eta\) chosen arbitrarily small. Fig. 2a shows the capacity region \(C(7, 6, 4, 4, 0, 0)\) (thick red line) and the \(\eta\)-NE region \(N_\eta(7, 6, 4, 4, 0, 0)\) (thin green line), with \(n_{11} \in \{0, 1, 2, 3, 4\}\) and \(n_{22} \in \{0, 1, 2, 3, 4\}\). Fig. 2b shows the capacity region \(C(7, 6, 4, 4, 5, 0)\) (thick red line) and the \(\eta\)-NE region \(N_\eta(7, 6, 4, 4, 5, 0)\) (thin green line), with \(n_{22} \in \{0, 1, 2, 3, 4\}\). Fig. 2c shows the capacity region \(C(7, 6, 4, 4, 6, 0)\) (thick red line) and the \(\eta\)-NE region \(N_\eta(7, 6, 4, 4, 6, 0)\) (thin green line), with \(n_{22} \in \{0, 1, 2, 3, 4\}\). Fig. 2d shows the capacity region \(C(7, 6, 4, 4, 7, 0)\) (thick red line) and the \(\eta\)-NE region \(N_\eta(7, 6, 4, 4, 7, 0)\) (thin green line), with \(n_{22} \in \{0, 1, 2, 3, 4\}\). Fig. 2e shows the capacity region \(C(7, 6, 4, 4, 7, 5)\) (thick red line) and the \(\eta\)-NE region \(N_\eta(7, 6, 4, 4, 7, 5)\) (thin green line). Fig. 2f shows the capacity region \(C(7, 6, 4, 4, 7, 6)\) (thick red line) and the \(\eta\)-NE region \(N_\eta(7, 6, 4, 4, 7, 6)\) (thin green line). Fig. 2g and Fig. 2h illustrate the achievable scheme for the equilibrium rate pair \((3, 4)\) and \((5, 4)\) in \(N_\eta(7, 6, 4, 4, 5, 0)\).

\(\eta\)-Nash region can be enlarged is presented in [7]. Fig. 2c shows the capacity region \(C(7, 6, 4, 4, 6, 0)\) (thick red line) and the \(\eta\)-NE region \(N_\eta(7, 6, 4, 4, 6, 0)\) (thin green line), with \(n_{22} \in \{0, 1, 2, 3, 4\}\). Fig. 2e shows the capacity region \(C(7, 6, 4, 4, 7, 5)\) (thick red line) and the \(\eta\)-NE region \(N_\eta(7, 6, 4, 4, 7, 5)\) (thin green line). Fig. 2f shows the capacity region \(C(7, 6, 4, 4, 7, 6)\) (thick red line) and the \(\eta\)-NE region \(N_\eta(7, 6, 4, 4, 7, 6)\) (thin green line). Fig. 2g and Fig. 2h illustrate the achievable scheme for the equilibrium rate pair \((3, 4)\) and \((5, 4)\) in \(N_\eta(7, 6, 4, 4, 5, 0)\).

\[n_{11} > 4\] and \(n_{22} \in \{0, 1, 2, 3, 4\}\) (Figures 2b, 2c and 2d), the resulting \(\eta\)-Nash region is strictly larger than in the previous case. A similar effect is observed in Figures 2e and 2f. This observation implies the existence of a threshold on each feedback parameter \(n_{11}\) and \(n_{22}\) beyond which the \(\eta\)-Nash region is enlarged. The exact values of \(n_{11}\) and \(n_{22}\) given a fixed tuple \((n_{11}, n_{22}, n_{12}, n_{21})\), beyond which the \(\eta\)-Nash region can be enlarged is presented in [7]. Figure 2g and Figure 2h show the coding schemes to achieve the rate pairs \((3, 4)\) and \((5, 4)\), respectively, when \(n_{11} = 5\) and \(n_{22} = 0\). In Figure 2g, note that common randomness is used by transmitter-receiver pair 2 to prevent transmitter-receiver pair 1 from increasing its individual rate. More specifically, the bits \(b_1, b_2, b_3, \ldots\) are known by both transmitter 2 and receiver 2. The use of common randomness is also observed in [8, 9] and [10]. Common randomness reflects a competitive behavior between both transmitter-receiver pairs. In Figure 2g, common randomness is not used by transmitter-receiver pair 2 and thus, transmitter-receiver pair 1 achieves a higher rate at an \(\eta\)-NE with respect to the previous example. This suggests a more altruistic behavior.

The \(\eta\)-NE region \(N_\eta\) without feedback, i.e., when \(n_{11} = 0\) and \(n_{22} = 0\) (Theorem 1 in [8]), is \(N_\eta(\vec{n}_{11}, \vec{n}_{22}, n_{12}, n_{21}, 0, 0)\). The \(\eta\)-NE region with perfect feedback i.e., \(\vec{n}_{11} = \max(n_{11}, n_{12})\) and \(\vec{n}_{22} = \max(n_{22}, n_{21})\) (Theorem 1 in [9]), is \(N_\eta(\vec{n}_{11}, \vec{n}_{22}, n_{12}, n_{21}, \max(n_{11}, n_{12}), \max(n_{22}, n_{21}))\). From the comments above, it is interesting to highlight the following inclusions:

\[N_\eta(\vec{n}_{11}, \vec{n}_{22}, n_{12} n_{21}, 0, 0) \subseteq \tag{12}\]
\[N_\eta(\vec{n}_{11}, \vec{n}_{22}, n_{12}, n_{21}, \vec{n}_{11}, \vec{n}_{22}) \subseteq \]
\[N_\eta(\vec{n}_{11}, \vec{n}_{22}, n_{12}, n_{21}, \max(n_{11}, n_{12}), \max(n_{22}, n_{21}))\],

for all \(\eta > 0\). The inclusions above might appear trivial, however, enlarging the set of actions often leads to paradoxes.
(Braess Paradox [11]) in which the new game possesses equilibria at which players obtain smaller individual benefits and/or smaller total benefit. Nonetheless, letting both transmitter-receiver pairs to use feedback does not induce this type of paradoxes with respect to the case without feedback.

IV. PROOFS

To prove Theorem 1, the first step is to show that a rate pair \((R_1, R_2)\), with \(R_1 < L_1\) or \(R_2 > U_2\) for at least one \(i \in \{1, 2\}\), is not achievable at an \(\eta\)-equilibrium for all \(\eta > 0\). That is,

\[
N_\eta \subseteq C \cap B_\eta.
\]  

(13)

The second step is to show that, for all \(\eta > 0\), any point in \(C \cap B_\eta\) can be achievable at an \(\eta\)-equilibrium. That is,

\[
N_\eta \supseteq C \cap B_\eta.
\]  

(14)

which proves the equality \(N_\eta = C \cap B_\eta\).

a) Proof of (13): The proof of Lemma 3 is followed by the following lemmas.

Lemma 1: A rate pair \((R_1, R_2) \in C\), with either \(R_1 < L_1\) or \(R_2 < L_2\) is not achievable at an \(\eta\)-equilibrium for all \(\eta > 0\).

Proof: The proof of Lemma 1 is presented in [7].

The intuition behind this proof is that the rate \(R_i = \left(\frac{1}{n_i} - n_{ij}\right)^+\) is always achievable independently of the coding scheme of transmitter-receiver pair \(j\). To achieve \(R_i = \left(\frac{1}{n_i} - n_{ij}\right)^+\) transmitter \(i\) uses the most significant bit-pipes, which are interference free, to transmit new bits at each channel use \(n\).

Lemma 2: A rate pair \((R_1, R_2) \in C\), with either \(R_1 > U_1\) or \(R_2 > U_2\) is not achievable at an \(\eta\)-equilibrium for all \(\eta > 0\).

Proof: The proof of Lemma 2 is presented in [7].

This proof is based on the fact that at an \(\eta\)-NE, transmitter \(j\) might re-transmit some of the bits previously transmitted by transmitter \(i\). The interference produced by those re-transmitted bits at receiver \(i\) can be eliminated if they were received interference free during previous channel uses. This allows transmitter \(i\) to use the bit-pipes interfered with by those re-transmitted bits to send new information bits at each channel use. The key point of this proof is to show that the maximum number of bits that can be re-transmitted at an \(\eta\)-NE is upper bounded.

b) Proof of (14): Consider a modification of the coding scheme with noisy feedback presented in [4], which combines rate splitting [12], block Markov superposition coding [13] and backward decoding [14]. The novelty with respect to [4] consists of allowing users to introduce common randomness as suggested in [8] and [9].

Consider without any loss of generality that \(N = N_1 = N_2\). Let \(W_i(t) \in \{1, 2, \ldots, 2^{N_{R_1}}\}\) and \(\Omega_i(t) \in \{1, 2, \ldots, 2^{N_{R_i}}\}\) denote the message index and the random message index sent by transmitter \(i\) during the \(t\)-th block, with \(t \in \{1, 2, \ldots, T\}\), respectively. Following a rate-splitting argument, assume that \(\left(W_i(t), \Omega_i(t)\right)\) is represented by the indices \(\left(W_{i,1}(t), \Omega_{i,1}(t) ; W_{i,2}(t), \Omega_{i,2}(t) ; W_{i,p}(t)\right) \subseteq \{1, 2, \ldots, 2^{N_{R_i}}\} \times \{1, 2, \ldots, 2^{N_{R_1}}\} \times \{1, 2, \ldots, 2^{N_{R_1}}\}\), where \(R_i = R_{i,C1} + R_{i,C2} + R_{i,P}\) and \(R_{i,R} = R_{i,R1} + R_{i,R2}\). The rate \(R_{i,R}\) is the number of transmitted bits that are known by both transmitter \(i\) and receiver \(i\) per channel use, and thus it does not have an impact on the information rate \(R_i\).

The codeword generation follows a four-level superposition coding scheme. The indices \(W_{i,C1}(t)\) and \(\Omega_{i,C}(t)\) are assumed to be decoded at transmitter \(j\) via the feedback link of transmitter-receiver pair \(j\) at the end of the transmission of block \(t - 1\). Therefore, at the beginning of block \(t\), each transmitter possesses the knowledge of the indices \(W_{i,C1}(t), \Omega_{i,1}(t) ; W_{i,C2}(t), \Omega_{i,2}(t)\). In the case of the first block \(t = 1\), the indices \(W_{i,C1}(0), \Omega_{i,1}(0) ; W_{i,C2}(0), \Omega_{i,2}(0)\) are assumed to be known by all transmitters and receivers. Using these indices both transmitters are able to identify the same codeword in the first code-layer. This first code-layer, which is common for both transmitter-receiver pairs, is a sub-codebook of \(2^{2N_{R_1} + R_{i,R1}}\) codewords. Denote by \(\mathbf{u}_i\left(W_{i,C1}(t), \Omega_{i,1}(t) ; W_{i,C2}(t), \Omega_{i,2}(t)\right)\) the corresponding codeword in the first code-layer. The second code-layer is chosen by transmitter \(i\) using \(\left(W_{i,C1}(t), \Omega_{i,1}(t) ; W_{i,C2}(t), \Omega_{i,2}(t)\right)\) from the second code-layer, which is a sub-codebook of \(2^{2N_{R_1} + R_{i,R1}}\) codewords corresponding to the codeword \(\mathbf{u}_i\left(W_{i,C1}(t), \Omega_{i,1}(t) ; W_{i,C2}(t), \Omega_{i,2}(t)\right)\). Denote by \(\mathbf{w}_i\left(W_{i,C1}(t), \Omega_{i,1}(t) ; W_{i,C2}(t), \Omega_{i,2}(t)\right)\) the corresponding codeword in the second code-layer. The third code-layer is chosen by transmitter \(i\) using \(\left(W_{i,C1}(t), \Omega_{i,1}(t) ; W_{i,C2}(t), \Omega_{i,2}(t)\right)\) from the third code-layer, which is a sub-codebook of \(2^{2N_{R_1} + R_{i,R1} + R_{i,R2}}\) codewords corresponding to the codeword \(\mathbf{w}_i\left(W_{i,C1}(t), \Omega_{i,1}(t) ; W_{i,C2}(t), \Omega_{i,2}(t)\right)\). The corresponding codeword in the third code-layer. The fourth code-layer is chosen by transmitter \(i\) using \(W_{i,P}(t)\) from the fourth code-layer, which is a sub-codebook of \(2^{2N_{R_1} + R_{i,R1} + R_{i,R2}}\) codewords corresponding to the codeword \(\mathbf{v}_i\left(W_{i,C1}(t), \Omega_{i,1}(t) ; W_{i,C2}(t), \Omega_{i,2}(t)\right)\). Denote by \(\mathbf{x}_i \left(W_{i,C1}(t), \Omega_{i,1}(t) ; W_{i,C2}(t), \Omega_{i,2}(t)\right)\) the corresponding codeword in the fourth code-layer. Finally, the codeword \(\mathbf{x}_i \left(W_{i,C1}(t), \Omega_{i,1}(t) ; W_{i,C2}(t), \Omega_{i,2}(t); W_{i,P}(t)\right)\) to be sent during block \(t \in \{1, 2, \ldots, T\}\) is a simple concatenation of the previous codewords, i.e., \(\mathbf{x}_i = (\mathbf{u}_i^T, \mathbf{v}_i^T, \mathbf{x}_i^T) \in \{0, 1\}^{T \times N}\), where the message indices have been dropped for ease of notation.

The decoder follows a backward decoding scheme. In the following, this coding scheme is referred to as a randomized Han-Kobayashi coding scheme with noisy feedback (R-HK-NOF) and it is described in [7]. The rest of the proof consists of showing that the R-HK-NOF coding scheme is capable of achieving an \(\eta\)-NE with \((R_1, R_2) \in C \cap B_\eta\) for all \(\eta > 0\), subject to a proper choice of the rates \(R_{i,R1}\) and \(R_{i,R2}\), for all \(i \in \{1, 2\}\).

Lemma 3: The achievable region of the randomized Han-Kobayashi coding scheme for the D-LD-IC-NOF is the set
of non-negative rates \( \left( R_{1,C1}, R_{1,R1}, R_{1,C2}, R_{1,R2}, R_{1,P}, R_{2,C1}, R_{2,R1}, R_{2,C2}, R_{2,R2}, R_{2,P} \right) \) that satisfy the following conditions for all \( i \in \{1, 2 \} \) and \( j \in \{1, 2 \} \setminus \{ i \} \):

\[
\begin{align*}
R_{j,C1} + R_{j,R1} & \leq \theta_{1,i} , \\
R_{i} + R_{j,C} + R_{i,R} & \leq \theta_{2,i} , \\
R_{j,C2} + R_{j,R2} & \leq \theta_{3,i}, \\
R_{i,P} & \leq \theta_{4,i}, \\
R_{i,P} + R_{j,C2} + R_{j,R2} & \leq \theta_{5,i} , \\
R_{i,C2} + R_{i,P} + R_{j,C2} + R_{j,R2} & \leq \theta_{7,i} ,
\end{align*}
\]

where,

\[
\begin{align*}
\theta_{1,i} = & (n_{ij} - (\max (\overline{n}_{ii}, n_{ij}) - \overline{n}_{ii}))^+, \\
\theta_{2,i} = & \max (\overline{n}_{ii}, n_{ij}) , \\
\theta_{3,i} = & \min (n_{ij}, (\max (\overline{n}_{ii}, n_{ij}) - \overline{n}_{ii}))^+, \\
\theta_{4,i} = & (\overline{n}_{ii} - n_{ij})^+, \\
\theta_{5,i} = & \max ( (\overline{n}_{ii} - n_{ij})^+, \\
& \min (n_{ij}, (\max (\overline{n}_{ii}, n_{ij}) - \overline{n}_{ii}))^+ ) , \\
\theta_{6,i} = & \min (n_{ij}, (\max (\overline{n}_{jj}, n_{ji}) - \overline{n}_{jj}))^+, \\
& \min ( (n_{jj} - \overline{n}_{jj})^+, (\overline{n}_{jj} - n_{ji})^+ ) + (\overline{n}_{ii} - n_{ij})^+, \\
\theta_{7,i} = & \min (n_{ij}, (\max (\overline{n}_{jj}, n_{ji}) - \overline{n}_{jj}))^+, \\
& \min ( (n_{jj} - \overline{n}_{jj})^+, (\overline{n}_{jj} - n_{ji})^+ ) + (\overline{n}_{ii} - n_{ij})^+ .
\end{align*}
\]

**Lemma 5:** Let \( \eta > 0 \) be fixed and let the rate tuple \( R = (R_{1,C} - \frac{\eta}{6}, R_{1,R} - \frac{\eta}{6}, R_{1,P} - \frac{\eta}{6}, R_{2,C} - \frac{\eta}{6}, R_{2,R} - \frac{\eta}{6}, R_{2,P} - \frac{\eta}{6}) \) be achievable by using the R-HK-NOF, with

\[
R_{i,C} + R_{i,P} + R_{j,C} + R_{j,R} = \max (\overline{n}_{ii}, n_{ij}) + \frac{2}{3}\eta,
\]

for all \( i \in \{1, 2 \} \). Then, the rate pair \( (R_1, R_2) \), with \( R_1 = R_{1,C} + R_{1,P} - \frac{\eta}{3} \) is achievable at an \( \eta \)-Nash equilibrium.

**Proof:** The proof of Lemma 5 is presented in [7].

The following lemma shows that all the rate pairs \( (R_1, R_2) \in C \cap B_\eta \) are achievable by the R-HK-NOF coding scheme at an \( \eta \)-NE, for all \( \eta > 0 \).

**Lemma 6:** Let \( \eta > 0 \) be fixed. Then, for all rate pairs \( (R_1, R_2) \in C \cap B_\eta \), there always exists at least one \( \eta \)-NE transmit-receive configuration pair \( (s^*_1, s^*_2) \in A_1 \times A_2 \) such that \( u_1(s^*_1, s^*_2) = R_1 \) and \( u_2(s^*_1, s^*_2) = R_2 \).

**Proof:** The proof of Lemma 6 is presented in [7].

This proof consists of showing that the set of inequalities in (15) and (17) leads to a set of rate pairs identical to \( C \cap B_\eta \). This concludes the proof of Theorem 1.

**V. CONCLUSIONS**

In this paper, the \( \eta \)-NE region of the D-LD-IC-NOF has been characterized for all \( \eta > 0 \). This region contains the \( \eta \)-NE region without feedback studied in [8] and is contained within the \( \eta \)-NE region with perfect channel-output feedback studied in [9].

**REFERENCES**


