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Generic resonator models for real-time synthesis of reed and brass instruments

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Summary
From accurate measurements of bore profiles of various reed and brass instruments, a common and simplified geometrical model made of three parts totaling seven geometrical parameters is proposed. From this geometry, it is shown that a good approximation of the input impedance can be obtained by a combination of two lumped elements gathered in series and parallel with a distributed element. Each element is approximated and discretized in order to end up with costless digital filters representing the impedance impulse response. These filters require the order of twenty multiplication/additions per sample and their coefficients are analytically expressed as functions of the geometrical parameters. The choice of the geometry and the time discretization schemes are validated both through comparison with continuous models and through the estimation of the geometrical parameters via a global optimization procedure, using measured input impedance curves.

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1. Introduction
This paper aims at providing simple, yet accurate, digital models of the input impedances of conical woodwinds and brass instruments, for use in the context of real-time sound synthesis.

Many studies have been devoted to the modeling of acoustic bores. In the context of the direct problem, consisting in calculating the input impedance from a measured geometry, Causse et al. [5], have shown a very good accordance between models and measurements in the case of brasses. In the context of the inverse problem, consisting in reconstructing a bore profile [1, 18] from measurement, many methods have been developed, some of them leading to commercial devices citekausel.

The underlying physical model of the instrument bore calls the use of transfer matrices representing the geometrical assembly constituting the instrument. Unfortunately, for many elements citebe1,scavone1,kergomard1, the conversion of the models [20] or the measurements [8] in terms of stable and costless digital filters usable for real-time sound synthesis is not straightforward. Most attempts, based on the wave variables representations [19, 21] have been devoted to the accurate digital modeling of specific elements and their assembly rather than on simplified models of the whole bore.

The scope of this paper is to focus on the synthesis rather than on the simulation point of view. Some specific requirements of the synthesis approach can be summarized as follows: The resonator of the instrument is just one part of the whole functioning model which also includes flow models and excitor-dynamics models (see e.g. [17] ). In this context, the success of a synthesis process is mostly based on a subjective judgement involving both playability and timbre naturalness. Finally, from a digital instrument design point of view, the simplicity of the model and its small number of degrees of freedom are important features which prevent the loss of generality and facilitates its handling and timbre extrapolation.

This paper investigates both the direct and inverse problems by providing digital impedance models fully defined from coarse and flexible geometries and by validating the use of these geometries and the discretization schemes from the analysis and synthesis of measured impedances.

The paper is organized as follows: Section 2 briefly presents the fine geometries of three saxophones and one trumpet and how they can be gathered into more global elements. In section 3, simplified digital models for conical bores and Bessel horns are presented and an assembly of the main bore and the mouthpiece, common to saxophones and brasses is proposed. Sec-
2. Simplified geometrical models

In this section, from geometrical measurements made by Nederveen [13] and Caussé, a simplified geometrical model of saxophone-like and brass-like instruments is presented.

2.1. Saxophone model

The left panels of figure 1 show in dotted lines, from top to bottom, the measured radii of tenor, alto, and soprano saxophone. The right panels show a blow up of the measured values on the first 0.2m. The stars correspond to the measured values (after Nederveen).

2.2. Trumpet model

The left panel of figure 2 shows in dotted lines, from top to bottom, the measured radii of tenor, alto, and soprano saxophone. The right panels show a blow up of left panel on the first 0.2m. The stars correspond to the measured values (after Caussé).

Figure 2. Bore profile of a trumpet. Vertical axis: radius, in m. Horizontal axis: length, in m. Right panel: blow-up of left panel on the first 0.2m. The stars correspond to the measured values (after Caussé).

3. Digital impedance models

3.1. Main bore models

Continuous input impedance models and their digital versions are presented in the case of conical bores and Bessel horns.

3.1.1. Saxophone bore

Continuous model: The main bore is assumed to be conical with input radius \( R_2 \), top angle \( \theta_2 \) and whose effective length \( L_2 \) corresponds to that of the first open tonehole. Its input impedance denoted \( Z_2 \) is classically written:

\[
Z_2 = Z_{c2} \frac{1}{j \tan(kL_2)} + \frac{1}{j k x_e}
\]

where \( x_e = R_2 / \sin(\theta_2 / 2) \) is the length of the missing part of the cone and \( Z_{c2} = \rho c / (\pi R_2^2) \) is the characteristic impedance. The wavenumber \( k = k(\omega) \) includes viscothermal losses [14].

For various lengths, top angles and input radii, using stepped cone models made of an association of one thousand small cylinders, it has been determined that the radius \( R \) used to compute the losses could be taken as the radius corresponding to the average losses while the losses in the term \( 1/(jk x_e) \) could be ignored:

\[
\frac{L_2}{R} = \int_{x_e}^{L_2+x_e} \frac{dx}{R(x)}
\]

which gives, since \( R(x) = R_2 x/x_e \):

\[
R = \frac{R_2}{\mu_2 x_e} \ln \left( 1 + \frac{L_2}{x_e} \right)
\]

where the control parameter \( \mu_2 \) is used as an additional mean to adjust the losses.

Discrete model: The digital model of the main conical bore is built according to [9]. The losses are modelled with a first order low-pass filter. If \( F_c \) is the sampling rate and \( z = \exp(i \omega / F_c) \), \( \exp(-2 j k L_2) \) is approximated by the filter: \( \frac{\mu_0}{1 - z^{-D}} z^{-B} \) and the element \( j k x_e \) is discretized with the bilinear transformation: \( j k x_e \simeq 2 F_c (1 - z^{-1})/(1 + z^{-1}) x_e / c. \)
3.1.2. Brass bore

It is assumed that the radius of the horn part of the bore is modelled by: \( R(x) = R_2 x^\nu / x^\nu \) and that this bore is prolonged by a cylindrical bore of length \( L_c \). The frequencies used for the matching correspond to those of the second and sixth impedance peaks.

The discussion is limited to the case \( \nu < 0 \). For positive values of \( \nu \), the input impedance of a cylindrical bore with length \( L_c \) is close to the asymptote \( Z_e \). The input radius \( R(x) \) is the asymptote. The input radius of the horn part of the bore, \( R(x) \), is denoted \( R_2 \).

**Continuous model:** In the divergent case (\( \nu > 0 \)), it is assumed that \( x_e \) is close to the asymptote \( x_a = 0 \). If \( k x_e \) is large, by ignoring the radiation impedance and denoting \( Z_e = \rho c / (\pi R_2^2) \) the characteristic impedance, the input impedance can be written as [6]:

\[
Z_e = jZ_c \tan \left( k(x_e + L_c - \nu \frac{\pi}{2}) \right)
\]  

(3)

This shows that for positive frequencies, the input impedance is a translated version of \(-\nu c / (4L_c)\) of the input impedance of a cylindrical bore with length \( L_c = l_c + x_e \).

As it has been done for the cone case, frequency-dependent losses are taken into account through a modification of the input radius of the horn part of the bore, yielding:

\[
R = \frac{x_e - x_a}{\int_0^x \frac{dx}{R(x)}} = \frac{R_2}{\mu_2} (1 + \nu)
\]

(4)

**Discrete model for \( \nu < 0 \):** It is worth noting that \( Z_e \) is the impedance of a cylindrical bore element with length \( L_c \) terminated at \( x_s \) in an element with a purely imaginary impedance: \( Z_t = jZ_c \tan(-\nu \pi / 2) \). Since for positive values of \( \nu \), \( Z_t \) is negative and the impulse response associated to \( Z_e \) contains increasing exponentials [20], only the case \( \nu < 0 \) can insure a passive discrete system and this is why the discrete time model is built first from the case \( \nu < 0 \).

For digital efficiency, it is proposed to terminate a cylinder of length \( L \) in a lumped element, the impedance of which is a derivative and the associated reflection coefficient is an all-pass filter. At low frequency, this termination acts as a length increase, the effect of which is to decrease the frequencies of the first peaks, therefore corresponding to the case \( \nu < 0 \).

Let \( C \) and \( P \) denote the dimensionless impedances of the cylinder and the termination, respectively:

\[
C = \frac{1 - \exp(-2jkL)}{1 + \exp(-2jkL)} \quad P = r_p j\omega
\]

(5)

The total impedance is:

\[
\tilde{Z}_e = Z_e - C + C/P
\]

(6)

In order to approximate \( Z_e \) with \( \tilde{Z}_e \), analytic expressions of \( r_p \) and \( L \) as functions of \( \nu \) and \( L_c \) can be obtained using the approximation: \( \arctan(x) \approx \frac{\pi}{2} \frac{x}{1+x^2} \) assuming frequency independent losses. The values of the parameters are determined so that the frequency of two selected peaks are the same for the continuous and the digital models.

**Discrete model for \( \nu > 0 \):** The digital impedance model corresponding to the case \( \nu > 0 \) is built by noticing that the impedance of a Bessel horn with \( \nu = 1 \) is the admittance of a cylinder (or the impedance of a closed cylinder, hence exhibiting a peak at zero frequency) to which is subtracted a low frequency approximation of this peak. Indeed, the input impedance is exactly given by:

\[
Z_e = \frac{1}{j \tan(kl_c)} - \frac{1}{jkl_c}
\]

(7)

This suggests to start from the admittance associated to the impedance model proposed for \( \nu < 0 \) (equation (6)) as the dimensionless impedance for \( \nu > 0 \) and to remove its zero frequency peak.

The peak at zero frequency is removed using a first order Taylor expansion of \( \tilde{Z}_e \) at \( \omega = 0 \) yielding a total impedance, denoted \( \tilde{Z}_b \) as:

\[
\tilde{Z}_b = \frac{1}{Z_e} - \frac{1}{d_0 + d_1 D}
\]

(8)

where \( D \) is the bilinear transform.

The coefficients \( d_0 \) and \( d_1 \) are determined analytically by considering the value of the impedance at zero frequency, that has to be real and positive and the derivative of the associated reflection function, that has to be zero in order to ensure continuity. The peak matching process used previously leads again to analytical solutions for \( r_p \) and \( L \).

Figure 4 shows, for \( \nu = 0.55 \), \( x_e = 0.5m \), \( x_s = 0.01m \), \( R_2 = 7mm \) and for frequency independent losses, the modulus of \( Z_e \) and \( \tilde{Z}_b \). The frequencies used for the matching correspond to those of the second and sixth impedance peaks.
3.2. Backbore and mouthpiece models

The backbore is modelled by a small conical element of length $L_1$ with input radius $R_1$ and top angle $\theta_1$. Its input impedance will be denoted $Z_1$ and is:

$$Z_1 = \frac{1}{Z_{c1} + \frac{1}{j\tan(kL_1) + \frac{1}{j\omega L_1}}} \tag{9}$$

where $x_{cc} = R_1 / \sin(\theta_1 / 2)$ is the length of the missing cone and $Z_{c1} = \rho c/(\pi R_1)$ is the characteristic impedance. Using a low frequency approximation $(j\tan(kL_1) \simeq j k L_1)$ and assuming frequency independent losses finally leads to:

$$Z_1 = Z_{c1} \frac{x_{cc}}{L_1 + x_{cc}} (G + j\omega \frac{L_1}{c} (1-G)) = Z_{c1} C_1 \tag{10}$$

which shows that the conicity of the bore is carried by the coefficient: $x_{cc}/(L_1 + x_{cc})$.

The mouthpiece is also modelled by a lossless short cylindrical element with length $L_0$ and radius $R_0$ with input impedance:

$$Z_0 = Z_{c0} j k L_0 = Z_{c0} C_0 \tag{11}$$

The derivations involved in $Z_0$ and $Z_1$ are discretized with the bilinear transform. The losses contained in $Z_1$ are taken into account by considering the value of $G$ for a given frequency, chosen as the resonance frequency $\omega_b$ of the whole mouthpiece, constituting a Helmholtz resonator. As it has been done for the main bores, for the sake of flexibility of the model, an additional control parameter $\mu_1$ is used in order to allow a better matching of real losses in the backbore.

3.3. Full bore model

In what follows, $S_2$ denotes the dimensionless digital impedance corresponding either to the conical bore or to the Bessel horn (Eqs. (1) and (8)).

Since $Z_{c2} > Z_{c2}$, the input impedance of the combination backbore/main bore simplifies as a serial combination of elements. In the same way, the total input impedance of the whole bore simplifies as a parallel combination of elements since $Z_{c0} \ll Z_{c1}$. Hence, the final model using dimensionless variables is:

$$Z_e = \frac{1}{Z_{c2}} \frac{1}{Z_{c2} S_2 + Z_{c1} C_1 + \frac{1}{Z_{c0}}} \tag{12}$$

Equation (12) shows that the combination mouthpiece/backbore acts as a Helmholtz resonator with a cavity volume $V_0$ such that $C_0/Z_{c2} = j\omega V_0 / (\rho c^2)$, terminated in the main bore. As a convention, the cavity of the Helmholtz resonator will be considered to be hemispherical, which allows to parametrize it with a unique radius $R_0$, yielding:

$$C_0 = \frac{Z_{c0}}{Z_{c2}} = j\omega \frac{2\pi R_0^3}{3\rho c^2} \tag{13}$$

For the saxophone case, up to the element of impedance $Z_1$, which mainly acts as a length correction at low frequencies, this model is similar to that discussed by Dalmont et al. [7]. It is also a simplified version of that discussed in [3] for the oboe case, where it is shown that the role of the backbore of impedance $Z_1$ is to improve the inharmonicity correction provided by the volume of impedance $Z_0$.

For direct use of a synthesis scheme such as that already presented by the same authors in [9], Eq. (12) is converted into a difference equation expressing at each sample $n$ the acoustic pressure $p_n(n)$ as function of $u_n(n)$ and the past values of $p_n$ and $u_n$. Each filter coefficient is expressed analytically with respect to the geometric parameters. The computation cost of the whole digital impedance model is 21 multiplications/additions per signal sample for the brass model and 17 for the saxophone model.

3.4. Examples

The top panel of figure 5 shows, for the tenor saxophone, the impedances obtained with the continuous and digital models. Geometrical values are obtained with the profile shown in figure 1 and are: $L_2 = 1.2m$, $R_2 = 7.35mm$, $\theta_2 = 3.17$, $L_1 = 56mm$, $R_1 = 6.5mm$, $\theta_1 = 1.74$. The volume $V_0$ corresponds exactly to the missing part of the main conical bore, yielding $R_0 = 19.3mm$. The differences between the continuous and the discrete models are not noticeable for both the amplitudes and the frequencies (for example, the frequency differences for the first and fifth peak are respectively 0.5Hz and 2Hz).

The bottom panel shows the same quantities for the trumpet. Geometrical values are obtained from the profile shown in figure 2 and are: $L_2 = 1.28m$, $R_2 = 5mm$, $\nu = 0.5$, $L_1 = 72mm$, $R_1 = 1.85mm$, $\theta_1 = 3.64$. The volume $V_0$ is estimated by measuring the cup volume, yielding $R_0 = 9.1mm$. In the continuous model, the main bore is splitted into a cylindrical bore ($L = 0.62m$) and a Bessel horn ($L = 0.66m$). The most noticeable difference between the continuous and the discrete models lies in the frequency and the height of the first impedance peak. The frequency difference is caused by the choice of the frequencies leading to the solution for $r_p$ and $L$, corresponding here to the second and sixth impedance peaks. For other significant peaks, the largest frequency difference is obtained for the fourth peak and is 4Hz.

4. Optimization of geometrical parameters

The aim of the optimization process is to provide the geometrical parameters involved in Eq. (12) from a measured impedance spectrum. The global optimization method used is an evolution strategy with covariance matrix adaptation (CMA-ES) [10], distributed under GNU Public Licence [22]. The optimization process consists in finding the set of parameters:

- $R_2$, $L_2$, $\mu_2$, $\theta_2$ or $\nu$, characterizing the main bore.
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• $R_1$, $L_1$, $\mu_1$, $R_0$, characterizing the backbore and mouthpiece.

According to Eq. (10), the conicity $\theta_1$ of the backbore is taken into account as a modification of $Z_{c_1}$. In addition to these parameters, since the dimensionless impedance model is normalized with respect to the radius of the main bore, an impedance gain $G_z$ is used to ensure a proper scaling with respect to the measurement. The optimization is constrained: the possible value of each geometrical parameter is bounded. These constraints insure that the global minimum of the cost function leading to geometrically relevant parameters is reached and that the approximations leading to Eq. 12 are satisfied.

The cost function has been chosen as:

$$\Lambda = \left( \int_{\omega_m}^{\omega_M} \frac{|Z_c(\omega)|^p - |Z_{mes}(\omega)|^p}{\omega} \ d\omega \right)^{1/p}$$

$Z_{mes}(\omega)$ is the measured impedance, $p$ is a real number ($p = 3$ in the examples). Its role is to emphasize the matching of the heights and frequencies of the highest impedance peaks. The frequencies $\omega_m$ and $\omega_M$ correspond either to the frequency range of the measurements or to a user-defined frequency bandwidth. Working on the modulus of the impedance rather than on the complete impedance allows to get rid of possible phase errors during the measurements.

Figure 6 shows the measured impedance of an alto saxophone and the digital impedance leading to the global minimum of the cost function. The minimisation has been performed on the whole frequency range available in the measure [20Hz - 1600Hz]. The estimated geometrical parameters are: $G_z = 1.5$, $L_2 = 0.97 m$, $R_2 = 6.61 mm$, $\mu_2 = 2.8$, $\theta_2 = 3.5$, $L_1 = 40 mm$, $R_1 = 5.52 mm$, $\mu_1 = 1$, $R_0 = 17.7 mm$. The Helmholtz resonance frequency is 770Hz and is close to the “break frequency” related to the cutoff frequency of the tonehole lattice measured in [4] (837Hz). The maximum amplitude and frequency errors correspond to the first peak and are $\Delta A/A = 25\%$ and $\Delta f/f = 1.5\%$, respectively. This is natural since the chosen value of $p$ emphasizes the accuracy of the estimation on the higher peaks. For the other peaks whose frequencies are below 1000Hz, the average $\Delta f/f$ is 0.13\% while the average $\Delta A/A$ is 11\%.

Figure 7 shows the measured impedance of a trumpet and the impedance yielding the global minimum of the cost function. The minimisation has been performed on the frequency range [140Hz - 1300Hz] and ignores the first impedance peak since it is not used during the play. The estimated geometrical parameters are: $G_z = 3.2$, $L_2 = 1.5 m$, $R_2 = 5.8 mm$, $\mu_2 = 2.6$, $\nu = 0.76$, $L_1 = 7.1 mm$, $R_1 = 1.51 mm$, $\mu_1 = 0.4$, $R_0 = 12.8 mm$. The Helmholtz resonance frequency is 815Hz. If the first peak is ignored, the maximum amplitude and frequency errors correspond to the second peak and are respectively $\Delta A/A = 25\%$ and $\Delta f/f = 0.9\%$. For the other peaks whose frequencies are below 1000Hz, the average $\Delta f/f$ is 0.2\% while the average $\Delta A/A$ is 5\%. This last value is smaller than in the saxophone case since all the peaks roughly have the same heights.

It can be noticed that, though the frequency and heights of the impedance peaks have been favored in the estimations, the values of the frequencies and amplitudes of the admittance peaks are also accurately reproduced below 1000Hz for both the trumpet and the saxophone. It has been checked that the difference above 1000Hz is due to the approximation of the backbore and the mouthpiece with lumped elements.
5. Conclusion

Flexible and numerically efficient digital impedance models can be found using the decomposition of bores of common instruments into three sections. Comparisons with continuous models show a very good accordance, even though drastic approximations to reduce the computation cost are made. The parameters of the digital models obtained from impedance measurements lead to a plausible instrument geometry and this validates the approximations made from the synthesis point of view.

Sound examples are available at:
http://www.lma.cnrs-mrs.fr/~guillemain/index.html

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References

[22] http://www.bionik.tu-berlin.de/user/niko